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Adaptive State-Quantized Control of Uncertain Lower-Triangular Nonlinear Systems with Input Delay

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Abstract: In this paper, we investigate the adaptive state-quantized control problem of uncertain lower-triangular systems with input delay. It is assumed that all state variables are quantized for the feedback control design. The error transformation method using an auxiliary time-varying signal is presented to deal with the compensation problem of input delay. Based on the error surfaces with the auxiliary variable, a neural-network-based adaptive state-quantized control scheme is constructed with the design of the input delay compensator. Different from existing results in the literature, the proposed method exhibits the following features: (i) compensating for the input delay effect by using quantized states; and (ii) establishing the stability of the adaptive quantized feedback control system in the presence of input delay. Furthermore, the boundedness of all the signals in the closed-loop and the convergence of the tracking error are analyzed. The effectiveness of the developed control strategy is demonstrated through the simulation on a hydraulic servo system.

Keywords: state-quantized control; neural network; input delay; uncertain triangular nonlinear systems



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1. Introduction

Owing to theoretical challenges and several practical applications, the feedback control problems of triangular nonlinear systems have been actively addressed in the control community (see [1–3] and references therein). Especially, as network-based industrial applications increase, input delays caused by the network transformation become unavoidable in the control system [4,5]. Therefore, the control design strategies for uncertain nonlinear systems with input delay have been developed. In [6–9], predictor-based control approaches are presented for nonlinear systems with input delay. A truncated-predictor-based control method has been studied for nonlinear systems with Lipschitz nonlinearities [10]. However, these results [6–10] only consider uncertain nonlinearities matched to the delayed control input. To deal with uncertain nonlinearities unmatched to the delayed control input, adaptive control design strategies using Pade approximation have been developed for uncertain triangular nonlinear systems with input delay [11–14]. In [15–19], input delay compensation approaches using the high-order auxiliary dynamics are presented to eliminate the influence of input delay on the recursive controller design. However, these studies do not consider the state quantization problem that is important with the input delay problem in network-based control environments with the communication channel bandwidth and limited computation resources. To the best of our knowledge, the state-quantized control problem of uncertain lower-triangular systems with input delay is still open.

The quantized control problem under capability-limited communication network is attracting much research attention recently, owing to extensive industrial applications [20,21]. To overcome the capability-limited communication problem, the quantization of all measured state variables is required to transmit state-feedback signals to the controller through the network. In this procedure, the quantization errors in the closed-loop cause control

performance degradation and even instability. Motivated by the above-mentioned issues, state-quantized control methods have been proposed for lower-triangular nonlinear systems with Lipschitz conditions [22,23]. To approximate unknown and unmatched nonlinearities in nonlinear systems, a neural-network-based quantized feedback control result is presented in [24]. This approach has been extended to nonlinear strict-feedback systems with state delays [25] where the Lyapunov–Krasovskii functional technique is employed to remove the effects of state delays. Despite these studies, the input delay problem has not been investigated in the quantized feedback control framework of triangular nonlinear systems. The main difficulty in dealing with input delay in the state-quantized control design is to provide the input delay compensator using quantized states and to analyze the stability of the closed-loop signals including the input delay compensator.

In this paper, we aim at addressing the adaptive state-quantized control problem in the presence of input delay in uncertain triangular nonlinear systems with unknown nonlinearities and external disturbances. The measured full states are quantized by state quantizers and the quantized states are only used to design the controller. Different from the existing quantized feedback control results [22–25], our primary contribution is to establish an input delay compensation strategy using quantized states in the state-quantized control framework while ensuring the robustness against unknown nonlinearities and external disturbances. To this end, an error coordinated transformation using the auxiliary variable is derived to design the delay compensator and the neural-network-based adaptive controller. An adaptive state-quantized control scheme is designed to guarantee the boundedness of all involved signals and the quantization errors. In the proposed control structure, the delay compensator and adaptive tuning laws based on quantized states are induced from the Lyapunov-based stability analysis methodology. It is shown that the control error is guaranteed to converge to a set that can be reduced as small as desired by adjusting design parameters. The simulation result on a hydraulic servo system is provided to demonstrate the effectiveness of the developed theoretical strategy.

The paper is organized as follows. In Section 2, the state-quantized control problem in the presence of input delay is formulated and the neural network approximation property is introduced. In Section 3, the adaptive state-quantized control scheme with a delay compensator and its closed-loop stability analysis are given. In Section 4, the simulation result on a hydraulic servo system is presented to illustrate the effectiveness of the state-quantized control scheme. Finally, the paper is concluded in Section 5.

2. Problem Formulation

In this paper, we consider the following class of uncertain lower-triangular nonlinear systems with input delay:

$$\begin{aligned} \dot{x}_i(t) &= x_{i+1}(t) + g_i(\bar{x}_i(t)) + \delta_i(t) \\ \dot{x}_n(t) &= u(t-d) + g_n(\bar{x}_n(t)) + \delta_n(t) \\ y(t) &= x_1(t) \end{aligned} \quad (1)$$

where $i = 1, \dots, n-1$, $\bar{x}_j = [x_1, \dots, x_j] \in \mathbb{R}^j$, $j = 1, \dots, n$, are the state variable vectors, $y \in \mathbb{R}$ denotes the system output, d is a non-negative input delay, $u(t-d) \in \mathbb{R}$ is the control input with input delay, δ_j , $j = 1, \dots, n$, are uncertain exogenous disturbances, and $g_j(\bar{x}_j) : \mathbb{R}^j \mapsto \mathbb{R}$, $j = 1, \dots, n$, are unknown C^1 nonlinear functions. The networked-based control problem with state quantization is considered in this paper. Then, all state variables x_j , $j = 1, \dots, n$, are quantized via the following uniform quantizer

$$Q(x_j) = \begin{cases} \rho_l, & \rho_l - \frac{\omega}{2} \leq x_j < \rho_l + \frac{\omega}{2} \\ 0, & -\frac{\omega}{2} \leq x_j < \frac{\omega}{2} \\ -\rho_l, & -\rho_l - \frac{\omega}{2} \leq x_j < -\rho_l + \frac{\omega}{2} \end{cases} \quad (2)$$

where $j = 1, \dots, n$, $l \in \mathbb{Z}^+$, ω is the quantization level, $\rho_1 = \omega$, and $\rho_{l+1} = \rho_l + \omega$. Then, the quantization error is defined as $\zeta_{x_j} \triangleq x_j - Q(x_j)$ that satisfies the property $|\zeta_{x_j}| \leq \omega$ [26].

Thus, $Q(x_j)$ instead of x_j are available for the design of the feedback control law u where $j = 1, \dots, n$.

The main objective of this paper is to design an adaptive tracking law u using quantized states $Q(x_j)$ for nonlinear systems (1) with input delay so that the system output y follows the desired signal y_r while all the closed-loop signals remain bounded where y_r, \dot{y}_r , and \ddot{y}_r are bounded.

Assumption 1. The disturbances δ_j are bounded as $|\delta_j| \leq \bar{\delta}_j$ where $j = 1, \dots, n$ and $\bar{\delta}_j$ are unknown constants.

In the proposed control scheme, the unknown nonlinear functions $g_j, j = 1, \dots, n$, are online approximated via the radial basis function neural networks (RBFNNs) over compact sets $\Xi_j \subset \mathbb{R}^j$ as follows [27]:

$$g_j(\bar{x}_j) = \Theta_j^\top B_j(\bar{x}_j) + \varepsilon_j(\bar{x}_j) \tag{3}$$

where $\bar{x}_j \in \Xi_j$ denotes an input vector, $\Theta_j \in \mathbb{R}^N$ is an ideal bounded weighting vector satisfying $\|\Theta_j\| \leq \bar{\Theta}_j$ with a constant $\bar{\Theta}_j$, ε_j denotes a reconstruction error satisfying $|\varepsilon_j| \leq \bar{\varepsilon}_j$ with a constant $\bar{\varepsilon}_j$, and $B_j = [b_{j,1}, \dots, b_{j,N}]^\top \in \mathbb{R}^N$ is the Gaussian function vector with elements $b_{j,m}(\bar{x}_j) = e^{-\|\bar{x}_j - c_{j,m}\|^2 / w_{j,m}^2}, m = 1, \dots, N$. Here, $c_{j,m} \in \mathbb{R}^j$ and $w_{j,m}$ are the center and width of the Gaussian functions, respectively.

Lemma 1. [28,29] The Gaussian basis function vector B_j is bounded as $\|B_j\| \leq \bar{B}_j$ with a constant \bar{B}_j .

3. Adaptive State-Quantized Tracking Control in the Presence of Input Delay

In this section, we design the neural-network-based adaptive state-quantized controller using the following coordinated transformation:

$$\begin{aligned} s_1 &= y - y_r \\ s_i &= x_i - \beta_{i-1,1}, \quad i = 2, \dots, n - 1 \\ s_n &= x_n - \beta_{n-1,1} - k_u \tanh \rho \\ \dot{\beta}_{m,1} &= \beta_{m,1} - v_m, \quad m = 1, \dots, n - 1 \end{aligned} \tag{4}$$

where $s_j, j = 1, \dots, n$, denote error surfaces, $k_u > 0$ is a design parameter, ρ is the auxiliary time-varying signal for compensating for the input delay effect, v_m are virtual controllers, and $\beta_{m,1}$ are the signals obtained by the following low-pass command filters

$$\begin{aligned} \dot{\beta}_{m,1} &= \beta_{m,2} \\ \dot{\beta}_{m,2} &= -2a_{m,1}a_{m,2}\beta_{m,2} - a_{m,2}^2(\beta_{m,1} - v_m) \end{aligned} \tag{5}$$

where $\beta_{m,1}(0) = v_m(0), \beta_{m,2}(0) = 0$, and $a_{m,1} > 0$ and $a_{m,2} > 0$ are design constants. Notice that the command filters (5) are employed based on the command filtered backstepping approach [3].

Remark 1. Compared with the existing adaptive control works for state-quantized nonlinear systems [22–25], this paper presents the error transformation method using the auxiliary variable ρ to deal with the input delay problem in the quantized feedback control framework. We design the input delay compensator using quantized states at the last design step and the stability analysis strategy of the total closed-loop system including this input delay compensator is presented in this paper. This is the main contribution of our study.

The controller design is presented from the Lyapunov-based recursive design step by step.

Step 1: Using (1) and (4), the dynamics of s_1 is defined as $\dot{s}_1 = x_2 + g_1 + \delta_1 - \dot{y}_r$. By considering a Lyapunov function $V_1 = (1/2)s_1^2$ and using (3), we have

$$\dot{V}_1 = s_1[s_2 + \tilde{\beta}_{1,1} + v_1 + \Theta_1^\top B_1(x_1) + \varepsilon_1 + \delta_1 - \dot{y}_r]. \tag{6}$$

Then, we choose the virtual control law v_1 as

$$v_1 = -k_1 s_1 - \hat{\Theta}_1^\top B_1(x_1) - \hat{\gamma}_1 \tanh\left(\frac{s_1}{\sigma_1}\right) + \dot{y}_r \tag{7}$$

where $k_1 > 0$ and $\sigma_1 > 0$ denote design constants, $\hat{\Theta}_1$ is the estimate of Θ_1 , and $\hat{\gamma}_1$ is the estimate of the unknown parameter $\tilde{\gamma}_1$ to be determined later.

Using (7), (6) becomes

$$\dot{V}_1 = -k_1 s_1^2 - s_1 \tilde{\Theta}_1^\top B_1(x_1) - s_1 \hat{\gamma}_1 \tanh\left(\frac{s_1}{\sigma_1}\right) + s_1(s_2 + \tilde{\beta}_{1,1} + \varepsilon_1 + \delta_1) \tag{8}$$

where $\tilde{\Theta}_1 = \hat{\Theta}_1 - \Theta_1$ is an estimation error vector.

Step i ($i = 2, \dots, n - 1$): Consider the Lyapunov function $V_i = (1/2)s_i^2$. Using (3)–(5), the time derivative of V_i is represented by

$$\dot{V}_i = s_i(s_{i+1} + \tilde{\beta}_{i,1} + v_i + \Theta_i^\top B_i(\bar{x}_i) + \varepsilon_i + \delta_i - \beta_{i-1,2}). \tag{9}$$

The virtual control law v_i is designed as

$$v_i = -k_i s_i - \hat{\Theta}_i^\top B_i(\bar{x}_i) - \hat{\gamma}_i \tanh\left(\frac{s_i}{\sigma_i}\right) + \beta_{i-1,2} \tag{10}$$

where $k_i > 0$ and $\sigma_i > 0$ denote design constants, $\hat{\Theta}_i$ is the estimate of Θ_i , and $\hat{\gamma}_i$ is the estimate of $\tilde{\gamma}_i$ to be constructed later.

Using (10), (9) is obtained as

$$\dot{V}_i = -k_i s_i^2 - s_i \tilde{\Theta}_i^\top B_i(\bar{x}_i) - \hat{\gamma}_i \tanh\left(\frac{s_i}{\sigma_i}\right) + s_i(s_{i+1} + \tilde{\beta}_{i,1} + \varepsilon_i + \delta_i) \tag{11}$$

where $\tilde{\Theta}_i = \hat{\Theta}_i - \Theta_i$ is an estimation error vector.

Step n : A Lyapunov function is defined as $V_n = (1/2)s_n^2$. Using (3)–(5), the time derivative of V_n is represented by

$$\dot{V}_n = s_n(u(t - d) + \Theta_n^\top B_n(\bar{x}_n) + \varepsilon_n + \delta_n - \beta_{n-1,2} - k_u(\cosh^2 \rho)^{-1} \dot{\rho}). \tag{12}$$

The input delay compensator is designed as

$$\dot{\rho} = \frac{\cosh^2 \rho}{k_u} (-p \tanh \rho + u(t - d) - u(t)) \tag{13}$$

where $p > 0$ is a design constant.

Substituting (13) into (12) and defining an un-quantized control signal v_n , we have

$$\dot{V}_n = s_n(u(t) - v_n) + s_n(v_n + \Theta_n^\top B_n(\bar{x}_n) + \varepsilon_n + \delta_n - \beta_{n-1,2} + p \tanh \rho). \tag{14}$$

Then, v_n is selected as

$$v_n = -k_n s_n - \hat{\Theta}_n^\top B_n(\bar{x}_n) - \hat{\gamma}_n \tanh\left(\frac{s_n}{\sigma_n}\right) + \beta_{n-1,2} \tag{15}$$

where $k_n > 0$ and $\sigma_n > 0$ denote design constants, $\hat{\Theta}_n$ is the estimate of Θ_n , and $\hat{\gamma}_n$ is the estimate of $\tilde{\gamma}_n$ to be constructed later.

Applying (15) into (14) yields

$$\dot{V}_n = -k_n s_n^2 - \tilde{\Theta}_n^\top B_n(\bar{x}_n) - \hat{\gamma}_n \tanh\left(\frac{s_n}{\sigma_n}\right) + s_n(u(t) - v_n) + s_n(\varepsilon_n + \delta_n + p \tanh \rho) \tag{16}$$

where $\tilde{\Theta}_n = \hat{\Theta}_n - \Theta_n$ is an estimation error vector.

For the design of the adaptive state-quantized control law u , we define error surfaces $s_{q,j}$, $j = 1, \dots, n$, using quantized states $Q(x_j)$ as

$$\begin{aligned} s_{q,1} &= Q(x_1) - y_r \\ s_{q,i} &= Q(x_i) - \beta_{q,i-1,1}, \quad i = 2, \dots, n-1 \\ s_{q,n} &= Q(x_n) - \beta_{q,n-1,1} - k_u \tanh \rho \end{aligned} \tag{17}$$

where $\beta_{q,i-1,1}$ and $\beta_{q,n-1,1}$ are the command filtered signals of state-quantized virtual controllers $v_{q,i-1}$ and $v_{q,n-1}$, respectively, and ρ is obtained using the input delay compensator (13). The state-quantized virtual controllers $v_{q,m}$ and actual controller u are designed as

$$v_{q,m} = -k_m s_{q,m} - \hat{\Theta}_m^\top B_m(Q(\bar{x}_m)) - \hat{\gamma}_m \tanh\left(\frac{s_{q,m}}{\sigma_m}\right) + \beta_{q,m-1,2} \tag{18}$$

$$u = -k_n s_{q,n} - \hat{\Theta}_n^\top B_n(Q(\bar{x}_n)) - \hat{\gamma}_n \tanh\left(\frac{s_{q,n}}{\sigma_n}\right) + \beta_{q,n-1,2} \tag{19}$$

where $m = 1, \dots, n-1$, $Q(\bar{x}_j) = [Q(x_1), \dots, Q(x_j)]^\top$, $j = 1, \dots, n$, $\beta_{q,0,2} = y_r$, and the adaptive laws for $\hat{\Theta}_j$ and $\hat{\gamma}_j$ are constructed as

$$\dot{\hat{\Theta}}_j = \lambda_{\Theta,j} [s_{q,j} B_j(Q(\bar{x}_j)) - \sigma_{\Theta,j} |s_{q,j}| \hat{\Theta}_j] \tag{20}$$

$$\dot{\hat{\gamma}}_j = \lambda_{\gamma,j} \left[s_{q,j} \tanh\left(\frac{s_{q,j}}{\sigma_j}\right) - \sigma_{\gamma,j} |s_{q,j}| \hat{\gamma}_j \right] \tag{21}$$

with $j = 1, \dots, n$, tuning matrices $\lambda_{\Theta,j} > 0$, tuning gains $\lambda_{\gamma,j} > 0$, and positive constants $\sigma_{\Theta,j}$ and $\sigma_{\gamma,j}$ for σ -modification. Here, based on (5), the command filters for $\beta_{q,m,1}$ and $\beta_{q,m,2}$ are designed as

$$\begin{aligned} \dot{\beta}_{q,m,1} &= \beta_{q,m,2} \\ \dot{\beta}_{q,m,2} &= -2a_{m,1} a_{m,2} \beta_{q,m,2} - a_{m,2}^2 (\beta_{q,m,1} - v_{q,m}) \end{aligned} \tag{22}$$

where $m = 1, \dots, n-1$, $\beta_{q,m,1}(0) = v_{q,m}(0)$, and $\beta_{q,m,2}(0) = 0$.

Remark 2. The proposed adaptive state-quantized control scheme consists of the virtual and actual controllers (18) and (19) with the delay compensator (13), adaptive laws (20) and (21), and command filter (22) using the quantized states $Q(x_j)$, $j = 1, \dots, n$. Compared with the existing control works for nonlinear lower-triangular systems with input delay [11–19], the state quantization problem is firstly considered in this paper. Thus, the stability analysis strategy of the closed-loop systems with the proposed adaptive state-quantized control scheme in the presence of input delay should be newly presented.

For the stability analysis, we present the following lemmas.

Lemma 2. If $\hat{\Theta}_j$ and $\hat{\gamma}_j$ are tuned via the adaptive laws (20) and (21), respectively, then: (i) $\tilde{\Theta}_j(t) \in \Pi_{\Theta,j}$, $\forall t \geq 0$, is ensured when $\tilde{\Theta}_j(0) \in \Pi_{\Theta,j}$; and (ii) $\tilde{\gamma}_j(t) \in \Pi_{\gamma,j}$, $\forall t \geq 0$, is ensured when $\tilde{\gamma}_j(0) \in \Pi_{\gamma,j}$ where $j = 1, \dots, n$, $\Pi_{\Theta,j} = \{\tilde{\Theta}_j \mid \|\tilde{\Theta}_j\| \leq \psi_{\Theta,j}\}$ with a constant $\psi_{\Theta,j}$, $\tilde{\gamma}_j = \hat{\gamma}_j - \tilde{\gamma}_j$, and $\Pi_{\gamma,j} = \{\tilde{\gamma}_j \mid |\tilde{\gamma}_j| \leq \psi_{\gamma,j}\}$ with a constant $\psi_{\gamma,j}$.

Proof. (i) A Lyapunov function $V_{\Theta,j} = (1/2)\tilde{\Theta}_j^\top \lambda_{\Theta,j}^{-1} \tilde{\Theta}_j$ is considered. Then, differentiating $V_{\Theta,j}$ with respect to time and using $\hat{\Theta}_j = \Theta_j + \tilde{\Theta}_j$, we have

$$\dot{V}_{\Theta,j} = \tilde{\Theta}_j^\top (s_{q,j} B_j(Q(\bar{x}_j)) - \sigma_{\Theta,j} |s_{q,j}| (\Theta_j + \tilde{\Theta}_j)). \tag{23}$$

Using $\|\Theta_j\| \leq \tilde{\Theta}_j$ and Lemma 1, we obtain

$$\dot{V}_{\Theta,j} \leq \|\tilde{\Theta}_j\| |s_{q,j}| (\bar{B}_j + \sigma_{\Theta,j} \tilde{\Theta}_j - \sigma_{\Theta,j} \|\tilde{\Theta}_j\|). \tag{24}$$

Then, it is ensured that $\dot{V}_{\Theta,j} \leq 0$ when $\|\tilde{\Theta}_j\| \geq \psi_{\Theta,j}$ with $\psi_{\Theta,j} = (\bar{B}_j + \sigma_{\Theta,j} \tilde{\Theta}_j) / \sigma_{\Theta,j}$. Thus, when $\tilde{\Theta}_j(0) \in \Pi_{\Theta,j}$, $\tilde{\Theta}_j(t) \in \Pi_{\Theta,j}, \forall t \geq 0$, is ensured.

(ii) By defining a Lyapunov function $V_{\gamma,j} = (1/(2\lambda_{\gamma,j})) \tilde{\gamma}_j^2$ and using $\hat{\gamma}_j = \gamma_j + \tilde{\gamma}_j$ and the property $|\tanh(\cdot)| \leq 1$, the time derivative of $V_{\gamma,j}$ is

$$\dot{V}_{\gamma,j} \leq |\tilde{\gamma}_j| |s_{q,j}| (1 + \sigma_{\gamma,j} \tilde{\gamma}_j - \sigma_{\gamma,j} |\tilde{\gamma}_j|). \tag{25}$$

By defining $\psi_{\gamma,j} \triangleq (1 + \sigma_{\gamma,j} \tilde{\gamma}_j) / \sigma_{\gamma,j}$, we know that $\dot{V}_{\gamma,j} \leq 0$ when $|\tilde{\gamma}_j| \geq \psi_{\gamma,j}$. Thus, $\tilde{\gamma}_j(t) \in \Pi_{\gamma,j}$ is ensured for all $t \geq 0$ provided that $\tilde{\gamma}_j(0) \in \Pi_{\gamma,j}$. \square

Lemma 3. Let us define the errors between the un-quantized signals and quantized signals in the closed-loop system as $\zeta_{s,j} = s_j - s_{q,j}$, $\zeta_{v,i} = v_i - v_{q,i}$, $\zeta_u = v_n - u$, $\zeta_{\beta,i,1} = \beta_{i,1} - \beta_{q,i,1}$, and $\zeta_{\beta,i,2} = \beta_{i,2} - \beta_{q,i,2}$ where $j = 1, \dots, n$ and $i = 1, \dots, n - 1$. Then, these errors are bounded as $|\zeta_{s,j}| \leq \chi_{s,j}$, $|\zeta_{v,i}| \leq \chi_{v,i}$, $|\zeta_u| \leq \chi_u$ and $\|\zeta_{\beta,i}\| \leq \chi_{\beta,i}$ where $\zeta_{\beta,i} = [\zeta_{\beta,i,1}, \zeta_{\beta,i,2}]^\top$, and $\chi_{s,j}$, $\chi_{v,i}$, and $\chi_{\beta,i}$ are constants.

Proof. We prove the boundedness of the quantization errors step by step.

(i) From $|x_1 - Q(x_1)| \leq \omega$ and $\zeta_{s,1} = s_1 - s_{q,1} = x_1 - Q(x_1)$, we have $|\zeta_{s,1}| \leq \chi_{s,1} \triangleq \omega$. Then, using (7) and (18), $\zeta_{v,1}$ becomes

$$\zeta_{v,1} = -k_1 \zeta_{s,1} - \hat{\Theta}_1^\top (B_1(x_1) - B_1(Q(x_1))) - \hat{\gamma}_1 \left[\tanh\left(\frac{s_1}{\sigma_1}\right) - \tanh\left(\frac{s_{q,1}}{\sigma_1}\right) \right]. \tag{26}$$

From Lemma 1 and $|\tanh(\cdot)| \leq 1$, we have $|B_1(x_1) - B_1(Q(x_1))| \leq 2\bar{B}_1$ and $|\tanh(s_1/\sigma_1) - \tanh(s_{q,1}/\sigma_1)| \leq 2$. Then, using Lemma 2, it is ensured that $\|\hat{\Theta}_1\| \leq \psi_{\Theta,1} + \tilde{\Theta}_1$ and $|\hat{\gamma}_1| \leq \psi_{\gamma,1} + \tilde{\gamma}_1$. Thus, $\zeta_{v,1}$ is bounded as $|\zeta_{v,1}| \leq \chi_{v,1}$ with $\chi_{v,1} = k_1 \chi_{s,1} + 2\bar{B}_1(\psi_{\Theta,1} + \tilde{\Theta}_1) + 2(\psi_{\gamma,1} + \tilde{\gamma}_1)$.

The vector forms of the command filters (5) and (22) are written as

$$\dot{\beta}_1 = \Gamma_1 \beta_1 + \Delta_1 v_1, \quad \dot{\beta}_{q,1} = \Gamma_1 \beta_{q,1} + \Delta_1 v_{q,1} \tag{27}$$

where $\beta_1 = [\beta_{1,1}, \beta_{1,2}]^\top$, $\beta_{q,1} = [\beta_{q,1,1}, \beta_{q,1,2}]^\top$, $\Gamma_1 = \begin{bmatrix} 0 & 1 \\ -a_{1,2}^2 & -2a_{1,1}a_{1,2} \end{bmatrix}$, and $\Delta_1 = [0, a_{1,2}^2]^\top$. Thus, we have

$$\dot{\zeta}_{\beta,1} = \Gamma_1 \zeta_{\beta,1} + \Delta_1 \zeta_{v,1}. \tag{28}$$

The solution of (28) is represented by

$$\zeta_{\beta,1}(t) = e^{\Gamma_1 t} \zeta_{\beta,1}(0) + \int_0^t e^{\Gamma_1(t-\tau)} \Delta_1 \zeta_{v,1}(\tau) d\tau. \tag{29}$$

Using $|\zeta_{v,1}| \leq \chi_{v,1}$, the invertible property of A_1 , and the inequality $\|e^{\Gamma_1 t}\| \leq \iota_{1,1} e^{-\iota_{1,2} t}$ with constants $\iota_{1,1} > 0$ and $\iota_{1,2} > 0$ [30], $\zeta_{\beta,1}$ is bounded as

$$\begin{aligned} \|\zeta_{\beta,1}(t)\| &\leq \iota_{1,1}\|\zeta_{\beta,1}(0)\| + \chi_{v,1}\|\Delta_1\|\|\Gamma_1^{-1}(I - e^{\Gamma_1 t})\| \\ &\leq \chi_{\beta,1} \end{aligned} \tag{30}$$

where $\chi_{\beta,1} = \iota_{1,1}\|\zeta_{\beta,1}(0)\| + \chi_{v,1}\|\Delta_1\|\|\Gamma_1^{-1}\|(1 + \iota_{1,1})\|$.

(ii) Using (4) and (17), we have $\zeta_{s,i} = x_i - Q(x_i) + \zeta_{\beta,i-1,1}$ where $i = 2, \dots, n - 1$. From $|x_i - Q(x_i)| \leq \omega$ and $|\zeta_{\beta,i-1,1}| \leq \chi_{\beta,i-1}$, $\zeta_{s,i}$ is bounded as $|\zeta_{s,i}| \leq \chi_{s,i} \triangleq \omega + \chi_{\beta,i-1}$. Then, $\zeta_{v,i}$ is given by

$$\zeta_{v,i} = -k_i \zeta_{s,i} - \hat{\Theta}_i^\top (B_i(\bar{x}_i) - B_i(Q(\bar{x}_i))) - \hat{\gamma}_i \left[\tanh\left(\frac{s_i}{\sigma_i}\right) - \tanh\left(\frac{s_{q,i}}{\sigma_i}\right) \right] + \zeta_{\beta,i-1,2}. \tag{31}$$

From the procedure similar to the previous step and $|\zeta_{\beta,i-1,2}| \leq \chi_{\beta,i-1}$, $\zeta_{v,i}$ is bounded as $|\zeta_{v,i}| \leq \chi_{v,i}$ with $\chi_{v,i} = k_i \chi_{s,i} + 2\bar{B}_i(\psi_{\Theta,i} + \bar{\Theta}_i) + 2(\psi_{\gamma,i} + \bar{\gamma}_i) + \chi_{\beta,i-1}$.

By applying the procedures (29)–(30) to $\zeta_{\beta,i} = \Gamma_i \zeta_{\beta,i} + \Delta_i \zeta_{v,i}$, and using the inequality $\|e^{\Gamma_i t}\| \leq \iota_{i,1} e^{-\iota_{i,2} t}$ with constants $\iota_{i,1} > 0$ and $\iota_{i,2} > 0$, we have $\|\zeta_{\beta,i}(t)\| \leq \chi_{\beta,i}$ where $i = 2, \dots, n - 1$, $\chi_{\beta,i} = \iota_{i,1}\|\zeta_{\beta,i}(0)\| + \chi_{v,i}\|\Delta_i\|\|\Gamma_i^{-1}\|(1 + \iota_{i,1})\|$, $\Gamma_i = \begin{bmatrix} 0 & 1 \\ -a_{i,2}^2 & -2a_{i,1}a_{i,2} \end{bmatrix}$, and $\Delta_i = [0, a_{i,2}^2]^\top$.

(iii) Using (4) and (17) gives $\zeta_{s,n} = x_n - Q(x_n) + \zeta_{\beta,n-1,1}$. Then, it holds that $|\zeta_{s,n}| \leq \chi_{s,n} \triangleq \omega + \chi_{\beta,n-1}$. ζ_u is obtained as

$$\zeta_u = -k_n \zeta_{s,n} - \hat{\Theta}_n^\top (B_n(\bar{x}_n) - B_n(Q(\bar{x}_n))) - \hat{\gamma}_n \left[\tanh\left(\frac{s_n}{\sigma_n}\right) - \tanh\left(\frac{s_{q,n}}{\sigma_n}\right) \right] + \zeta_{\beta,n-1,2}. \tag{32}$$

From the procedure similar to the previous step and $|\zeta_{\beta,n-1,2}| \leq \chi_{\beta,n-1}$, ζ_u is bounded as $|\zeta_u| \leq \chi_u$ with $\chi_u = k_n \chi_{s,n} + 2\bar{B}_n(\psi_{\Theta,n} + \bar{\Theta}_n) + 2(\psi_{\gamma,n} + \bar{\gamma}_n) + \chi_{\beta,n-1}$. \square

Let us define the total Lyapunov function V as $V = \sum_{j=1}^n V_j + \sum_{m=1}^{n-1} \tilde{\beta}_m^\top F_m \tilde{\beta}_m$ where $\tilde{\beta}_m = [\tilde{\beta}_{m,1}, \beta_{m,2}]^\top$ and $F_m > 0$ denotes a symmetric matrix.

Theorem 1. Consider the system (1) with input delay controlled by the adaptive state-quantized control scheme (18)–(22) with the input delay compensator (13). For any initial conditions satisfying $V(0) \leq \mu$ with a constant $\mu > 0$, the control error s_1 is guaranteed to converge to a set that can be adjusted by design parameters while all the closed-loop signals remain bounded.

Proof. The dynamics of $\tilde{\beta}_m$ is represented by

$$\dot{\tilde{\beta}}_m = \Gamma_m \tilde{\beta}_m + c \Phi_m \tag{33}$$

where $m = 1, \dots, n - 1$, $c = [1, 0]^\top$, and

$$\begin{aligned} \Phi_1(Z_1) &= k_1 s_1 + \hat{\Theta}_1^\top B_1 + \hat{\Theta}_1^\top \dot{B}_1 + \hat{\gamma}_1 \tanh\left(\frac{s_1}{\sigma_1}\right) + \hat{\gamma}_1 \operatorname{sech}^2\left(\frac{s_1}{\sigma_1}\right) \frac{\dot{s}_1}{\sigma_1} - \ddot{y}_r \\ \Phi_i(Z_i) &= k_i s_i + \hat{\Theta}_i^\top B_i + \hat{\Theta}_i^\top \dot{B}_i + \hat{\gamma}_i \tanh\left(\frac{s_i}{\sigma_i}\right) + \hat{\gamma}_i \operatorname{sech}^2\left(\frac{s_i}{\sigma_i}\right) \frac{\dot{s}_i}{\sigma_i} - \dot{\beta}_{i-1,2}, \quad i = 2, \dots, n - 1 \end{aligned}$$

with $Z_1 = [s_1, s_2, \beta_{1,1}, \hat{\Theta}_1, \hat{\gamma}_1, y_r, \dot{y}_r, \ddot{y}_r, \delta_1]^\top$ and $Z_i = [s_1, \dots, s_{i+1}, \beta_{1,1}, \dots, \beta_{i,1}, \beta_{1,2}, \dots, \beta_{i-1,2}, \hat{\Theta}_1, \dots, \hat{\Theta}_i, \hat{\gamma}_1, \dots, \hat{\gamma}_i, y_r, \dot{y}_r, \ddot{y}_r, \delta_1, \dots, \delta_i]^\top$.

Substituting (8), (11), (16), and (33) into the time derivative of \dot{V} yields

$$\begin{aligned} \dot{V} &\leq - \sum_{j=1}^n k_j s_j^2 + \sum_{m=1}^{n-1} \tilde{\beta}_m^\top (F_m \Gamma_m + \Gamma_m^\top F_m) \tilde{\beta}_m + \sum_{j=1}^{n-1} s_j (s_{j+1} + \tilde{\beta}_{j,1}) + \sum_{m=1}^{n-1} 2\tilde{\beta}_m^\top F_m c \Phi_m \\ &\quad + \sum_{j=1}^n s_j \gamma_j - \sum_{j=1}^n s_j \hat{\gamma}_j \tanh\left(\frac{s_j}{\sigma_j}\right). \end{aligned} \tag{34}$$

where $\gamma_i = \varepsilon_i + \delta_i - \tilde{\Theta}_i^\top B_i, i = 1, \dots, n - 1$, and $\gamma_n = \varepsilon_n + \delta_n - \tilde{\Theta}_n^\top B_n - \zeta_u + p \tanh \rho$.

From Lemmas 1–3, Assumption 1, and $|\varepsilon_j| \leq \bar{\varepsilon}_j$, there exist constants $\tilde{\gamma}_j$ such that $|\gamma_j| \leq \tilde{\gamma}_j$ with $j = 1, \dots, n$. Thus, we have $|s_j| \tilde{\gamma}_j - s_j \tilde{\gamma}_j \tanh(s_j/\sigma_j) \leq 0.2785 \tilde{\gamma}_j \sigma_j$. In addition, due to the Hurwitz matrix Γ_m , there exists the matrix $W_m > 0$ such that $F_m \Gamma_m + \Gamma_m^\top F_m = -W_m$. Then, (34) becomes

$$\begin{aligned} \dot{V} \leq & - \sum_{j=1}^n k_j s_j^2 - \sum_{m=1}^{n-1} w_m \tilde{\beta}_m^\top \tilde{\beta}_m + \sum_{j=1}^{n-1} s_j (s_{j+1} + \tilde{\beta}_{j,1}) + \sum_{m=1}^{n-1} 2 \tilde{\beta}_m^\top F_m c \Phi_m \\ & - \sum_{j=1}^n s_j \tilde{\gamma}_j \tanh\left(\frac{s_j}{\sigma_j}\right) + \sum_{j=1}^n 0.2785 \tilde{\gamma}_j \sigma_j. \end{aligned} \tag{35}$$

where w_m denotes a minimum eigenvalue of W_m .

From the boundedness of $\hat{\Theta}_j, \hat{\gamma}_j$, and $\delta_j, j = 1, \dots, n$, there exist functions $\Phi_i^*, i = 1, \dots, n - 1$, such that

$$\begin{aligned} |\Phi_1(Z_1)| & \leq \Phi_1^*(s_1, s_2, \beta_{1,1}, y_r, \dot{y}_r, \ddot{y}_r) \\ |\Phi_m(Z_m)| & \leq \Phi_m^*(s_1, \dots, s_{m+1}, \beta_{1,1}, \dots, \beta_{m,1}, \beta_{1,2}, \dots, \beta_{m-1,2}, y_r, \dot{y}_r, \ddot{y}_r) \end{aligned} \tag{36}$$

where $m = 2, \dots, n - 1$. Consider the compact sets $\Omega_i, i = 1, \dots, n - 1$, and Ω_{y_r} as $\Omega_i = \{(s_1, \dots, s_{i+1}, \tilde{\beta}_1, \dots, \tilde{\beta}_i) : \sum_{h=1}^{i+1} s_h^2 + \sum_{h=1}^i 2 \tilde{\beta}_h^\top F_h \tilde{\beta}_h \leq 2\mu\}$ and $\Omega_{y_r} = \{(y_r, \dot{y}_r, \ddot{y}_r) : y_r^2 + \dot{y}_r^2 + \ddot{y}_r^2 \leq \mu_r\}$, respectively, where $\mu_r > 0$ is a constant. From (36), it holds that $|\Phi_i^*| \leq \bar{\Phi}_i$ on $\Omega_i \times \Omega_{y_r}$ where $\bar{\Phi}_i$ is a constant. Using the inequalities $s_j s_{j+1} \leq s_j^2/2 + s_{j+1}^2/2, s_j \tilde{\beta}_{j,1} \leq s_j^2/2 + \|\tilde{\beta}_j\|^2/2, 2 \tilde{\beta}_m^\top F_m c \Phi_m \leq (\Phi_m^*)^2 \|F_m\|^2 \|\tilde{\beta}_m\|^2/\vartheta + \vartheta$, and $-s_j \tilde{\gamma}_j \tanh(s_j/\sigma_j) \leq s_j^2/2 + \psi_{\gamma,j}^2/2$ with a constant $\vartheta > 0$, and choosing $k_1 = 3/2 + \bar{k}_1, k_j = 2 + \bar{k}_j, k_n = 3/2 + \bar{k}_n, w_m = 1/2 + \bar{\Phi}_m^2 \|F_m\|^2/\vartheta + \bar{w}_m$ with constants $\bar{k}_1 > 0, \bar{k}_j > 0, \bar{k}_n > 0$, and $\bar{w}_m > 0$, (35) becomes

$$\dot{V} \leq - \sum_{j=1}^n \bar{k}_j s_j^2 - \sum_{m=1}^{n-1} \bar{w}_m \tilde{\beta}_m^\top \tilde{\beta}_m - \sum_{m=1}^{n-1} \left(1 - \frac{(\Phi_m^*)^2}{\bar{\Phi}_m^2}\right) \frac{\bar{\Phi}_m^2 \|F_m\|^2 \|\tilde{\beta}_m\|^2}{\vartheta} + O_1 \tag{37}$$

with $O_1 = \sum_{j=1}^n (\psi_{\gamma,j}^2/2 + 0.2785 \tilde{\gamma}_j \sigma_j) + (n - 1)\vartheta$. Because of $|\Phi_i^*| \leq \bar{\Phi}_i$ on $V = \mu$, (37) becomes

$$\dot{V} \leq -O_2 V + O_1 \tag{38}$$

with $O_2 = \min[2\bar{k}_1, \dots, 2\bar{k}_n, \bar{w}_1/f_1, \dots, \bar{w}_n/f_n]$. Here, $f_j, j = 1, \dots, n$, denotes the maximum eigenvalue of F_j . (38) implies that $\dot{V} < 0$ on $V = \mu$ provided that $O_2 > O_1/\mu$. Therefore, $V \leq \mu$ is an invariant set. It is ensured that all closed-loop signals are semi-globally uniformly ultimately bounded. Thus, the control input u is bounded. From the solution of (38), the control error s_1 converges to a compact set $\Omega_{s_1} = \{s_1 | |s_1| \leq \sqrt{2O_1/O_2}\}$ that can be reduced by increasing O_2 . Then, we check the boundedness of the input compensator ρ in (13). Using the boundedness of s_j and $\tilde{\beta}_m$ and Lemmas 2 and 3, $s_{q,n}$ and $\beta_{q,n-1,2}$ are bounded. Thus, u is bounded. Then, there exists a constant \bar{q} such that $|u(t - d) - u(t)| \leq \bar{q}$. Owing to $(\cosh^2 \rho)/k_u \geq 0, \rho$ is bounded. \square

Remark 3. From the proof of Theorem 1, the control design parameters are selected to reduce the compact set Ω_{s_1} . Thus, the guidelines are presented as follows:

- (i) Decreasing the quantization level ω helps to decrease O_1 . This leads to reduce Ω_{s_1} .
- (ii) Selecting fixed small constants $\sigma_{\Theta,j}$ and $\sigma_{\gamma,j}$ and increasing $\lambda_{\Theta,j}, \lambda_{\gamma,j}$, and $k_j, j = 1, \dots, n$ help to increase O_2 , which subsequently reduces Ω_{s_1} .
- (iii) The eigenvalues of W_m can be adjusted by the parameters $a_{m,1}$ and $a_{m,2}$ of the command filters $i = 1, \dots, n$. Thus, increasing w_m helps to decrease Ω_{s_1} .

Remark 4. This paper provides a theoretical basis for the adaptive state-quantized control design of uncertain lower-triangular systems with input delay. Based on the proposed control approach, the following topics can be recommended as future works.

(i) Nonlinear stochastic systems in lower-triangular forms have been studied in the adaptive neural control field (see [31–33] and references therein). Based on these works, an adaptive state-quantized neural tracking control problem of nonlinear stochastic systems can be considered as a future topic. To apply the proposed approach to nonlinear stochastic systems, the analysis methodologies of the quantization errors of virtual and actual control laws should be newly developed based on some technical lemmas dealing with nonlinear stochastic systems. Then, such a future topic can be extended to adaptive state-quantized control problems of uncertain pure feedback stochastic nonlinear systems with state constraints and nonlinear stochastic switched lower triangular systems with input saturation.

(ii) The nonlinear systems concerned in this paper are in the lower-triangular form. To apply the proposed state-quantized control approach to non-lower triangular nonlinear systems, the well known technical lemma [34] on the radial basis function of the neural network (i.e., $\|B_j(\bar{x}_n)\| \leq \|B_j(\bar{x}_j)\|$) can be used in the proposed control design steps. Based on this lemma, the state-quantized control problem of non-lower triangular structure with unknown input saturation can be investigated as a future topic.

4. Simulation

4.1. Example 1

To show the effectiveness of the proposed adaptive state-quantized control system in the presence of input delay, we consider a practical nonlinear model of a hydraulic servo system with input delay and compare our controller with the existing quantized feedback controller [24] designed without considering input delay. The nonlinear model of a hydraulic servo system is represented by [35]:

$$\begin{aligned} c_m \ddot{\phi}(t) + c_d \dot{\phi}(t) + c_s \phi(t) &= D_F(t) + \omega(t) \\ \frac{v_c}{4b_e} \dot{H}_p(t) + L_f H_p(t) + R \dot{\phi}(t) &= S_I(t - d) \end{aligned} \tag{39}$$

where ϕ and P_L denote the displacement of the inertia load and the pressure difference of the hydraulic actuator, respectively; the driving force D_F is defined as $D_F = RH_p$ with the ram area R ; ω is the friction inside the cylinder; c_m , c_d , and c_s indicate the load mass, the damping constant, and the spring constant, respectively; v_c , b_e , and L_f are the effective bulk modulus of oil, the volume of the cylinder, and the total internal leakage factor, respectively; S_I denotes the supply input flow; and d is the input delay.

Using the form of (1), the state-space model of (39) is given by

$$\begin{aligned} \dot{x}_1(t) &= x_2(t) \\ \dot{x}_2(t) &= x_3(t) + g_2(\bar{x}_2(t)) + \delta_2(t) \\ \dot{x}_3(t) &= u(t - d) + g_3(\bar{x}_3(t)) \end{aligned} \tag{40}$$

where $x_1 = \phi$, $x_2 = \dot{\phi}$, $x_3 = RH_p/c_m$, $u = 4Rb_e S_I/(c_m v_c)$, $g_2 = -(c_d/c_m)x_2 - (c_s/c_m)x_1$, $\delta_2 = (1/c_m)\omega$, and $g_3 = -4(b_e/v_c)L_f x_3 - 4(R^2 b_e/(c_m v_c))x_2$. The system parameters are taken from [35]. The friction disturbance is set to $\delta_2(t) = 0.1 \cos(0.5t)$. To solve the differential equation (40) for this simulation, we use the fourth-order Runge–Kutta method with the step size 0.005 within 50 s. The initial conditions are set to $\bar{x}_3(0) = [0.2, 0, 0]^T$. The desired signal y_r is defined as $y_r = 0.1 \cos(0.6t + \pi/3)$. The quantization level and the input delay are set to $\omega = 0.001$ and $d = 0.08$, respectively. The adaptive state-quantized control scheme for the system (40) is given by the virtual and actual controller (18) and (19) with the delay compensator (13), adaptive laws (20) and (21), and command filter (22). The control parameters are selected as $k_1 = k_2 = k_3 = 10$, $\lambda_{\Theta,j} = 20$, $\lambda_{\gamma,j} = 5$, $\sigma_{\Theta,j} = \sigma_{\gamma,j} = 0.01$, $p = 20$, $k_u = 50$, $a_{1,1} = 10$, $a_{2,1} = 70$, $a_{m,2} = 0.707$, and $\sigma_j = 0.5$ where $j = 2, 3$ and $m = 1, 2$.

The quantized-states-based control results and errors are compared in Figure 1. As shown in Figure 1, while the divergent system output and tracking error are provided via

the previous controller presented in [24], the convergent system output and tracking error are provided via the proposed state-quantized controller. Thus, the previous controller presented in [24] cannot ensure the stability of the closed-loop system in the presence of input delay. The adaptive tuning parameters for the proposed approach are shown in Figure 2. In Figure 3, the response of the input compensator and the control input are displayed. In these figures, we can see that the proposed state-quantized controller has good tracking performance for input-delayed nonlinear systems with state quantization.

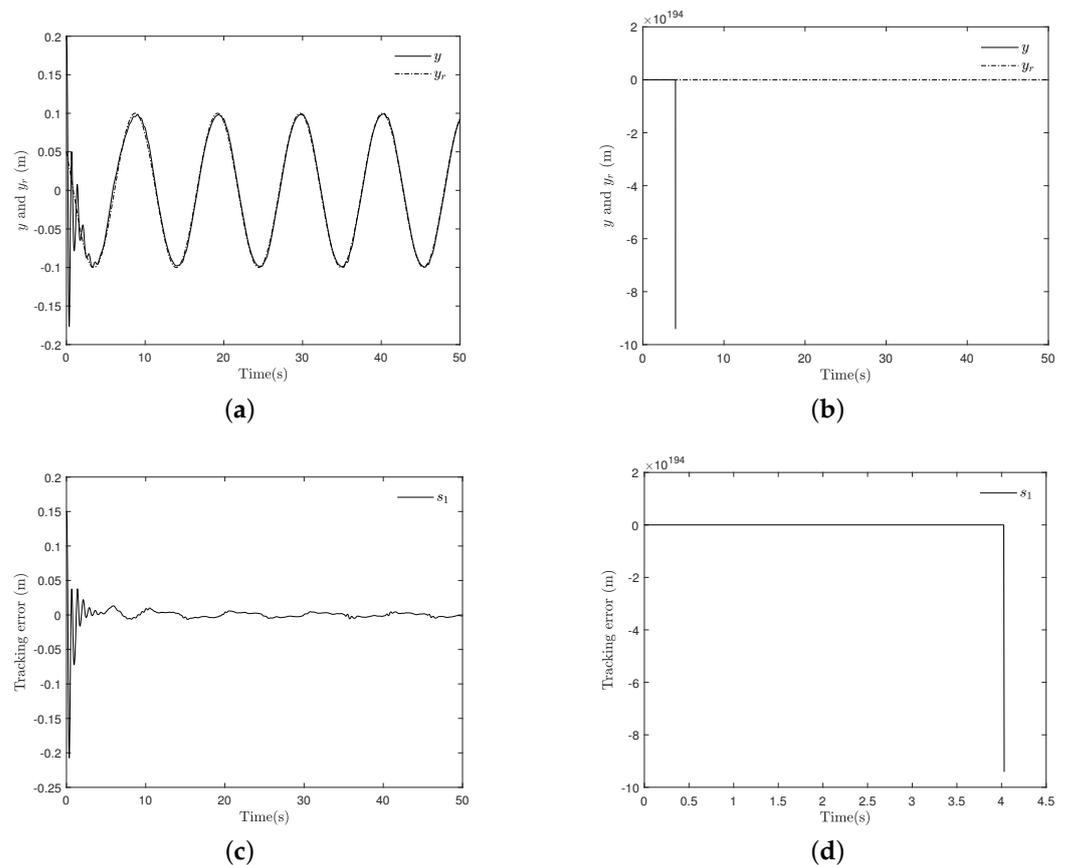


Figure 1. Comparison of tracking results and errors for Example 1: (a) y and y_r of the proposed control system; (b) y and y_r of the control system presented in [24]; (c) s_1 of the proposed control system; and (d) s_1 of the control system presented in [24].

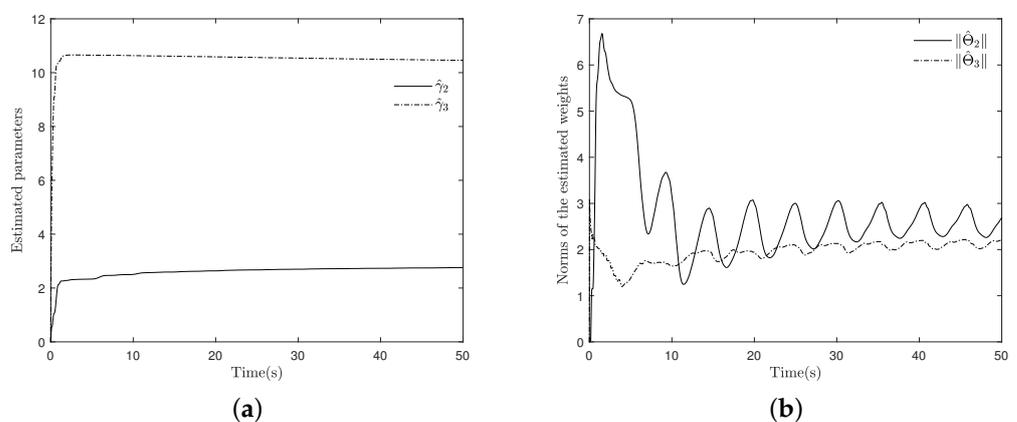


Figure 2. Estimation results of the proposed control system for Example 1 (a) $\hat{\gamma}_j, j = 2, 3$; and (b) $\|\hat{\theta}_j\|, j = 2, 3$.

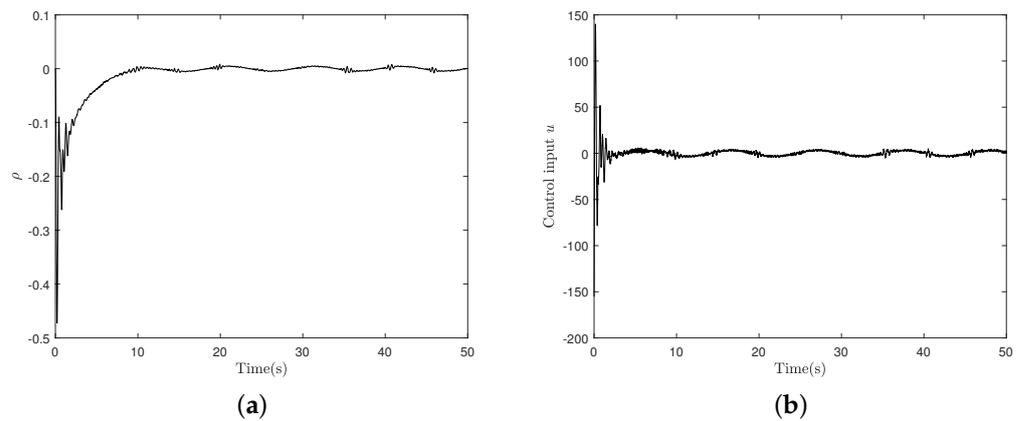


Figure 3. Input delay compensator and control input of the proposed control system for Example 1: (a) ρ ; and (b) u .

4.2. Example 2

Consider the following nonlinear systems:

$$\begin{aligned} \dot{x}_1(t) &= x_2(t) + g_1(x_1(t)) + \delta_1(t) \\ \dot{x}_2(t) &= x_3(t) + g_2(x_2(t)) + \delta_2(t) \\ \dot{x}_3(t) &= u(t-d) + g_3(x_3(t)) + \delta_3(t) \end{aligned} \tag{41}$$

where $g_1 = 0.5x_1^2 \cos x_1$, $g_2 = e^{-x_1^2}x_2 + 0.2 \cos(0.5x_2)$, $g_3 = x_1x_3 + x_2 \sin x_3$, and $\delta_1 = \delta_2 = \delta_3 = 0.1 \sin(0.2t)$. Using the fourth-order Runge–Kutta method with the step size 0.005 within 30 s, the differential equation (41) is solved for this simulation. The initial conditions are set to $\bar{x}_3(0) = [0.5, 0, 0]^T$. The desired signal y_r is defined as $y_r = 0.4 \cos(0.7t)$. The quantization level and the input delay are set to $\omega = 0.01$ and $d = 0.05$, respectively. The design parameters are set to $k_1 = 1$, $k_2 = 10$, $k_3 = 30$, $\lambda_{\Theta,j} = 10$, $\lambda_{\gamma,j} = 5$, $\sigma_{\Theta,j} = 0.01$, $\sigma_{\gamma,j} = 0.1$, $p = 10$, $k_u = 50$, $a_{m,1} = 40$, $a_{m,2} = 0.707$, and $\sigma_j = 0.5$ where $j = 1, 2, 3$.

In Figure 4, the tracking control results and errors of the proposed approach and the previous controller [24] are compared. While the system output and tracking error of the previous controller [24] diverge, those of the proposed state-quantized controller converge. Therefore, the proposed adaptive state-quantized tracking approach can be used in the presence of input delay. Figure 5 shows the adaptive estimated parameters of the proposed state-quantized controller. Figure 6 displays the response of the input compensator and the control input of the proposed state-quantized controller. It is observed that all the closed-loop signals are bounded and the state-quantized tracking is successfully achieved in the presence of input delay.

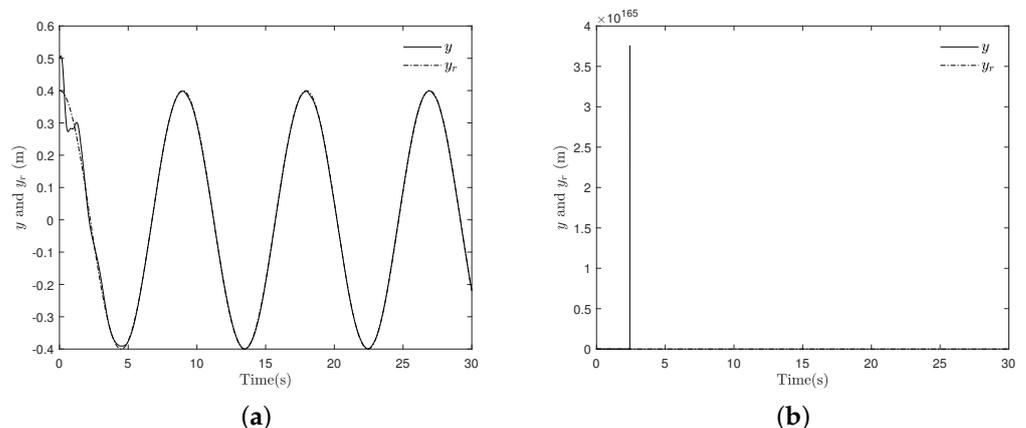


Figure 4. Cont.

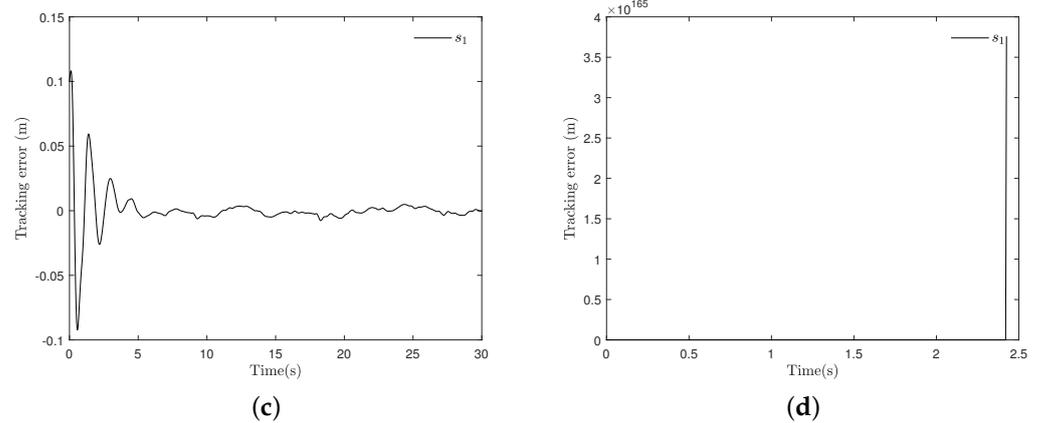


Figure 4. Comparison of tracking results and errors for Example 2: (a) y and y_r of the proposed control system; (b) y and y_r of the control system presented in [24]; (c) s_1 of the proposed control system; and (d) s_1 of the control system presented in [24].

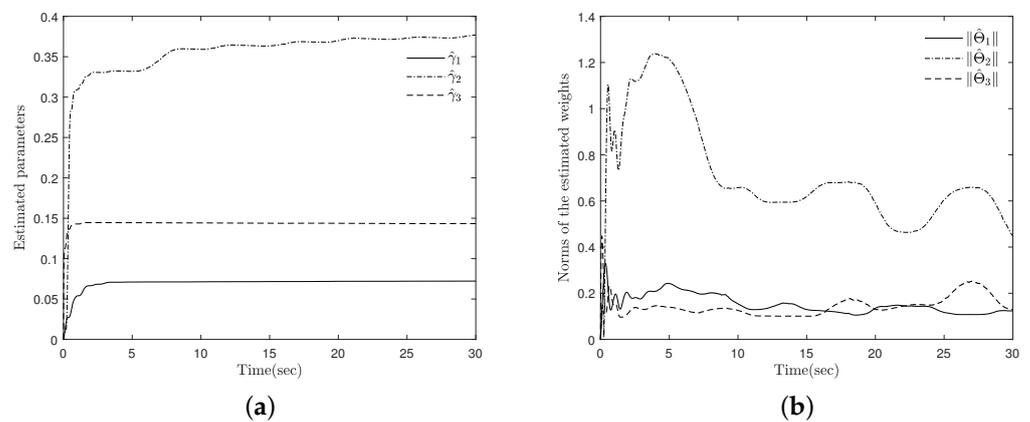


Figure 5. Estimation results of the proposed control system for Example 2: (a) $\hat{\gamma}_j, j = 1, 2, 3$; and (b) $\|\hat{\theta}_j\|, j = 1, 2, 3$.

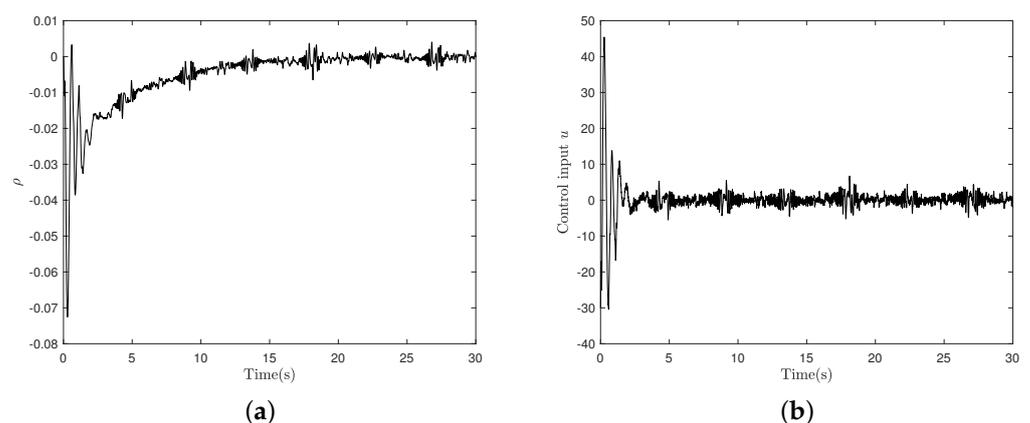


Figure 6. Input delay compensator and control input of the proposed control system for Example 2: (a) ρ ; and (b) u .

5. Conclusions

This paper develops the adaptive state-quantized control strategy to compensate for the input delay of uncertain nonlinear lower-triangular systems with state quantization. The error surface using the auxiliary time-varying signal for compensating for the input delay is derived for the control design. A neural-network-based adaptive controller and

its adaptive laws are constructed via quantized states while designing the input delay compensator using quantized states. In the proposed control scheme, the quantization errors and approximation errors are compensated via the adaptive technique and their boundedness is analyzed by establishing some technical lemmas. All involved signals are ensured to be bounded. The effectiveness of the proposed approach is demonstrated by the hydraulic servo dynamics. Compared with the existing quantized feedback control designs of nonlinear systems, the primary contribution of this paper is to provide the adaptive state-quantized control strategy in the presence of input delay. This paper provides a theoretical basis for the adaptive state-quantized control design in the presence of input delay. Thus, the proposed approach can be extended to various practical systems in the lower-triangular form such as aircraft wing rock models, jet engines, flight systems, biochemical processes, and flexible-joint robots reported in [1].

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